

Motorola Semiconductor Application Note

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Precision Sine-Wave Tone Synthesis Using 8-Bit MCUs

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Introduction

The pervasive nature of the modern microcontroller (MCU) has resulted in numerous products that now contain one or more MCUs as central subsystems. Cell phones, base stations, repeaters, SLICs (subscriber line interface cards), and cordless telephones are just a few of the many products which have MCUs at the center of their functionality.

These products also require precision tone generators for functions such as dual-tone-multi-frequency signaling (DTMF), call progress tones, continuous tone-coded squelch system encode (CTCSS), digital continuous tone-coded squelch system encode (DCTCSS), and user interface chimes.

While off-the-shelf components generally are available for these functions, the added cost can be greatly reduced by using the already present MCU to synthesize the desired tones. This benefit is multiplied in systems where many unrelated tone protocols are required, since the same synthesis firmware/hardware can be used across a wide range of frequencies.

This application note presents basic tone synthesis techniques and illustrates their implementation using the HC08, HC05, HC11, and HC12 Families of MCUs.



Tone Synthesizer Basics

When an analog signal is stored in digital memory, an A/D (analog-to-digital) converter is used to provide quantized samples at a specific data rate (known as the sample rate or F_S) to be stored in memory as binary values. To retrieve the stored signal, the binary samples are extracted from memory and sent to a D/A (digital-to-analog) converter at the same rate at which they were stored. As long as the analog signal has no frequency components greater than half the sample rate (as per the Nyquist criteria), the reconstructed signal will appear to closely follow the original waveform. (Quantization effects in the A/D will introduce some errors.)

To generate a tone at a specific frequency, one can simply digitize a sample of the tone to be reconstructed and store the sample in the system memory for later recall. However, for a multi-tone system, each tone requires a separate sample and thus its own memory storage. The more tone frequencies required, the more storage needed to hold the samples. In addition, the sample lengths for different frequencies will not be consistent, since each stored sample must continue until the signal repeats. This method would be tedious to maintain, use large amounts of memory to store relatively few tones, and would be limited to only those tones which were stored previously.

Another reconstruction method would be to generate a single sample and vary the reconstruction sample rate. This would produce a signal with a variable frequency with only one stored cycle, but it would yield a variable and non-linear F_{step} (F_{step} is the smallest, non-zero increment of frequency).

As an example, consider an 8-MHz master clock and a 256-byte sine sample. The 8-MHz master clock is applied to a programmable 16-bit divider which is used to set the sample rate. To obtain reconstructed tones from near-DC to 3 kHz, the divider would range from 65535 ($8E6 / 65535 / 256 = 0.477$ Hz) to 10 ($8E6 / 10 / 256 = 3.125$ kHz).

At the low end of the frequency range, the Fstep would be:

$$\begin{aligned} \text{Fstep} &= \text{Fdiv2} - \text{Fdiv1} \\ &= (8\text{E6} / 65534 / 256) - (8\text{E6} / 65535 / 256) \\ &= 0.47685 - 0.47684 \\ &= 0.00001 \text{ Hz} \end{aligned}$$

While at the high end:

$$\begin{aligned} \text{Fstep} &= \text{Fdiv2} - \text{Fdiv1} \\ &= (8\text{E6} / 10 / 256) - (8\text{E6}/11 / 256) \\ &= 3125 - 2841 \\ &= 284 \text{ Hz} \end{aligned}$$

This illustrates that the example would exhibit an Fstep variation of several orders of magnitude across the signal passband. Not only would this complicate real-time frequency calculations on the target system, but the Fstep granularity at the higher frequencies would severely limit the utility of the system. (Typically, Fstep should be at least 0.5 Hz across the passband for most applications.)

Filtering this system would also pose some problems. A reconstruction filter (for instance, a low-pass filter with a cutoff frequency, F_c , just below the Nyquist rate of $F_s / 2$) is used to remove the PWM (pulse width modulation) sample frequency and higher order harmonics. If the sample rate is varied, the user must undertake the difficult and expensive task of designing a tunable filter that can track the sample rate so that the reconstructed signal can have a flat response in the passband. This would require additional hardware, MCU resources, and firmware support which would increase the cost of both development and production.

Direct Look-Up Synthesis

The direct-look-up synthesis algorithm described here uses a combination of the aforementioned schemes to produce precision waveforms across a specific frequency band. A look-up table holds a replica of the waveshape which is to be generated. (Typically, this is a mathematically generated sine table with N entries.) At every sample point, the algorithm uses the value of a phase accumulator to extract

data from the table which is sent to the D/A. The phase accumulator is a software register used to keep a "running total" of the current phase value of the synthesized signal. The algorithm also updates the phase accumulator to be used at the next sample point by adding a "delta phase" value, or Delta.

NOTE: *Look-up table accesses are modulo-N, such that any access beyond the end of the table will wrap-around to the beginning.*

To obtain finer Fstep granularity, Delta and the phase accumulator are represented as fractional quantities with the integer portion being used as the index into the sine table.

The frequency of the resulting tone can be deduced by setting Delta = 1. At every sample point, the integer portion of the phase accumulator is incremented by exactly 1. Since this corresponds to the index into the sine table, the D/A output simply will follow the sine table. Since the table holds one cycle, the frequency of the output will be 1/tgen, where tgen is the time required for one full cycle.

With N table entries sent at 1/Fs per entry:

$$tgen = N * 1 / Fs.$$

If Delta is doubled, the table will be cycled in half the samples, which results in:

$$tgen = N / (2Fs)$$

Thus, tgen is inversely proportional to the value of Delta. Since $F = 1/t$, the frequency of the generated signal is given by this equation:

$$(1) \quad Fgen = (Fs * Delta) / N$$

As noted, Delta is a fractional quantity valid in this range:

$$0 \leq Delta < N / 2$$

For microcontroller applications, Delta is most easily represented as a 2-byte quantity (referred to here as Dreg) with the upper byte holding the integer portion and the lower byte holding the fractional portion (thus, the

radix lies between bits 7 and 8). The decimal value of Delta would be represented as:

$$(2) \quad \Delta = \text{Dreg}[15:0] / \text{mod}(\text{fractional})$$

Since the fractional portion is represented here as an 8-bit value, $\text{mod}(\text{fractional}) = 256$ which yields:

$$(3) \quad \Delta = \text{Dreg}[15:0] / 256$$

and

$$\text{Dreg}[15:0] = 256 * \Delta$$

The 16-bit Dreg value is thus added to the 16-bit phase accumulator at each sample period to generate the table index and running phase reference. The table index is extracted from the phase accumulator by masking the integer portion with $N - 1$ (valid for $N = 2^x$, where x is a positive integer). For an 8-byte table, the mask would be $\$07$ (the lower three bits) and for a 256-byte table the mask would be $\$FF$ (all eight bits of the integer portion of Delta). This provides a simple and efficient method of implementing the numerical values used to represent Delta.

Example:

$$\text{Given: } N = 8, F_s = 8 \text{ kHz, and } F_{\text{gen}} = 800 \text{ Hz}$$

From equation 1, solve for Delta,

$$\begin{aligned} \Delta &= (N * F_{\text{gen}}) / F_s \\ &= (8 * 800) / 8000 \\ &= 0.8 \end{aligned}$$

The integer and fractional parts (high byte/low byte) are represented as:

$$\text{Integer} = 0$$

$$\text{Fractional} = 0.8 * 256 = 204.8 \text{ (round to the nearest integer)} = \$CD$$

$$\text{Dreg} = \$00CD$$

The pointer mask, as noted, would be Accum[10:8] = [111], which is used as an offset into the 8-byte sine table.

**Table 1. Example of a 4-Bit, Unsigned Sine Table
($D/A = 8 + \text{int}(\sin(2\pi x / 16) * 15)$)**

Offset, x	D/A	Degrees
0	8	0
1	13	45
2	15	90
3	13	135
4	8	180
5	2	225
6	0	270
7	2	315

**Table 2. Example of Phase Accumulator History
(Each Line = 1 Sample Period)**

Accum [15:0]	Accum [10:8]	D/A Value from Table
\$0000	\$00	\$08
\$00CD	\$00	\$08
\$019A	\$01	\$0D
\$0267	\$02	\$0F
\$0334	\$03	\$0D
\$0401	\$04	\$08
\$04CE	\$04	\$08
:	:	:
:	:	:

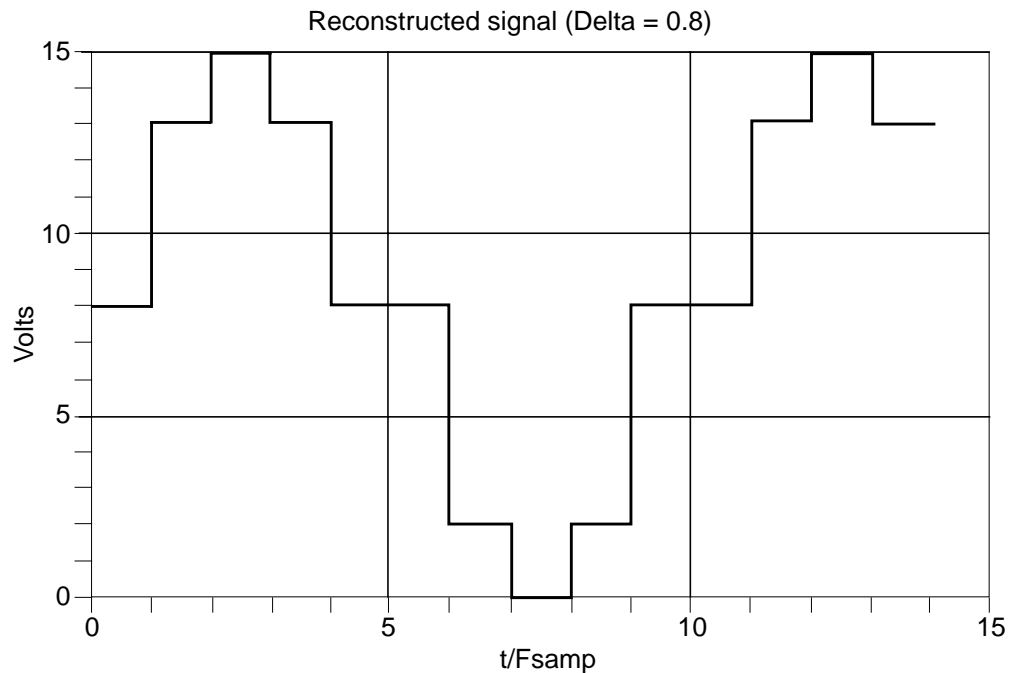


Figure 1. Delta = 0.8 (800 Hz) Example Using 8-Byte Table

Figure 1 illustrates a full cycle of the reconstructed signal, with each horizontal division representing one sample period ($1 / F_s = 1 / 8000 = 125 \mu\text{s}$). From this, the period of the waveform can be calculated by counting the number of sample periods for a full cycle and multiplying by the sample period (in this case, 10 samples = 1.25 ms = 1 / 800 Hz).

As is apparent from the plot of **Figure 1**, a table length of 8 results in a coarse reconstruction; a longer sine table gives more resolution and reduces harmonic distortion. Since the integer portion of Delta is eight bits, a 256-byte table is easily indexed while not reserving an excessive amount of memory. Linear interpolation can be used to increase accuracy with a shorter table, but this is generally not feasible on most MCUs due to processor bandwidth limitations. (However, the HC12 can support this method as is described later in this application note.)

An interesting result of this reconstruction method is that the relationship between Delta and F_s is linear, with each unit change in Delta resulting in the same change in F_{gen} across the entire pass-band. This value was

referred to earlier as F_{step} and represents the smallest possible change in F_{gen} .

F_{step} can be found from equations 1 and 3 by:

$$F_{step} = F_1 - F_2$$

Choose F_1 and F_2 :

$$F_1 = (F_s * D_{reg} / 256) / N$$

$$F_2 = (F_s * (D_{reg} - 1) / 256) / N$$

$$\begin{aligned} F_{step} &= ((F_s * D_{reg} / 256) / N) - (F_s * (D_{reg} - 1) / 256) / N \\ &= F_s / (256 * N) * (D_{reg} - (D_{reg} - 1)) \end{aligned}$$

$$(4) \quad F_{step} = F_s / (256 * N)$$

Thus, for any value of D_{reg} , the F_{step} is always equal to $F_s / (256 * N)$. One result worth consideration is that for a given sample rate, the only remaining variable to determine F_{step} is the table length.

From the previous example, $F_s = 8000$ Hz and $N = 8$, which gives $F_{step} = 3.906$ Hz. Increasing the table size to $N = 256$ results in $F_{step} = 0.122$ Hz. F_{step} specifies the maximum gross frequency error for any given tone frequency allowing system accuracy within $\pm F_{step}/2$ of any desired frequency.

After signal purity considerations, F_{step} typically is the next most important design parameter as it determines how accurately generic tone frequencies can be generated. Generally, a designer is faced with the need to generate tones over a specific frequency range with some degree of accuracy. Typically, this is specified in terms of %error (plus or minus) of the desired frequency, but also may be expressed as $\pm \Delta F$ (Hz). (Of course, specifying the error in this manner is trivial because $F_{step} < 2\Delta F$ is all that is required for the design to meet the specification.)

For systems that express error in terms of percent, use this equation to determine the maximum allowed Fstep:

$$(5) \quad F_{\text{step(max)}} = (F_{\text{min}} * \% \text{error}) / 2$$

Where F_{min} is the minimum desired frequency to be generated

Of course, this equation represents the design minimum, and usually it is desirable to choose as small an Fstep as is practical. Actual Fstep should be at least 50 percent of Fstep (max) from equation (5) to allow for round-off errors and normal variations in system clock frequency.

Dual Tone (Chord) Synthesis

Applications such as DTMF and call progress signaling require dual tone synthesis which is simply the generation of two mixed tones of unrelated frequencies. The term "chord" is sometimes used to describe this technique, even though the two tones are not necessarily related by harmonics. In direct look-up synthesis, dual tone generation is a straightforward extension of the single tone case described earlier. Two separate tones can be generated by maintaining two separate Dreg and phase accumulator registers. For each sample period, the system adds Dreg1 to accumulator1 and Dreg2 to accumulator2. The index extracted from each accumulator is used to separately extract D/A values from the same look-up table. Before sending to the D/A, however, these two values are added in software, with the resulting D/A output representing the algebraic sum of the two unrelated tones.

When mixing two signals on the same D/A channel in this manner, it is important to avoid overflow. Overflow occurs when a value is calculated that exceeds the D/A maximum range. If the two signals are of the same amplitude, the range of instantaneous amplitude can vary from a minimum of 0 to a maximum of $2A$, where A is the maximum amplitude of the individual signals. Thus, the maximum allowed value is $D/A(\text{max}) = 2A$, or $A = D/A(\text{max}) / 2$.

This can most easily be accomplished by "pre-dividing" the sine table values by 2 so that when any two values are summed, the result won't overflow the D/A.

While pre-division minimizes the real-time effort required by the firmware, it also increases the round-off error (because the D/A LSB

(least significant bit) of the original sine table values are lost). A better method is to use the original table and perform the division in real time (post-division). While this adds some overhead to the system, it reduces round-off error which results in improved dynamic range.

With an 8-bit D/A implementation on an 8-bit MCU, the most efficient way to implement post-division is to simply add the byte values and perform an ROR instruction on the result (divide by 2). When the two 8-bit values are added, the carry becomes the ninth bit. The effect of the ROR instruction is to divide this 9-bit value by two with the 8-bit result being the desired D/A value. While the LSB of the final D/A result is lost, it should be noted that this represents only one round-off error instead of the two errors introduced by the pre-division method.

Look-Up Table Requirements

The length of the look-up table is a primary design variable and is determined by available memory and desired Fstep resolution. D/A dynamic range also contributes to the length of the table as some systems can accommodate 10-, 12-, or 16-bit D/A sub-systems. This mandates more memory to hold the longer D/A values in the look-up table.

Another factor in determining table length derives from the nature of the accumulator/pointer system employed. To reduce firmware overhead, the look-up table length should be an exponential multiple of 2 (given earlier as $N = 2^x$). This simplifies the modulo bit mask to extract the D/A pointers which can save several execution cycles in code that is typically very time sensitive. Optimally, an 8-bit mask is chosen because this requires no extra cycles to extract the pointer which results in a code-optimal table length of 2^8 or 256 bytes. While this may result in an Fstep which is much smaller than required for some applications and increase the table memory required, the reduction in execution cycles can overshadow memory availability concerns in systems where ancillary firmware load is high.

D/A Methods

Two of the most popular D/A methods are direct conversion and pulse width modulation (PWM, also referred to as pulse length modulation, PLM). While direct D/A is the easier to implement (in terms of firmware support) and can result in less distortion and noise than PWM methods, typically, it is more expensive and therefore not as desirable in cost-sensitive systems.

For this reason, the bulk of the following discussion focuses on PWM methods for some of the 8- and 16-bit Motorola microcontrollers. In general, buffered PWM is preferred over non-buffered because the signal-to-noise ratio of the output can be adversely affected by even slight timing variations in the PWM signal.

Filtering

The sample frequency should be as high as possible (relative to the reconstructed signal) to relax the filtering requirements. The lower the sample frequency, the sharper the filtering required to effectively eliminate the stop-band frequency components. Some of the PWM methods described here are limited to carrier frequencies of around 8 kHz or less (due to timer and/or MCU clock speed limits), which can require very sharp filtering to sufficiently remove the PWM carrier and signal aliases from the D/A output for some applications.

Sample rate and filter order are the prime cost factors in a synthesis system. As the sample rate is increased, more D/A performance is required which typically increases costs by forcing the designer to exercise one or more of these choices:

- Use a higher frequency crystal
- Use a PWM module only available on a more expensive MCU
- Use an external D/A

The filter costs also are related to sample rate, but are inversely proportional, which has the effect of countering the cost issues. Thus, it usually is possible for the designer to reach a cost compromise which allows the system performance specifications to be met.

To approach the issue of filtering, the user first must consider the spectral content of the signal that is to be filtered. Sampling theory dictates that when a continuous time signal is sampled at a regular rate (for example, a sine wave), the spectrum of the reconstructed signal will be comprised of the spectrum of the original signal plus the original spectrum translated to harmonics of the sample frequency as illustrated in **Figure 2**. To recover the original signal, minus the translated spectra, a reconstruction filter is needed as indicated in the figure.

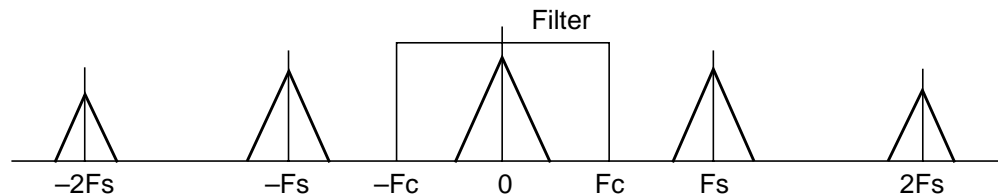


Figure 2. Reconstructed Signal Spectra and Filter Response ($F_c = \pm F_s/2$)

The ideal filter described in **Figure 2** would pass all signals below F_c , and reject all signals above F_c . Unfortunately, it is impossible to construct an ideal filter, which forces the designer to consider real filter performance when designing a synthesis system. The impact of this can be seen in **Figure 3** which shows a synthesized signal, F_{gen} ($F_{gen} < F_s/2$), inside a real filter passband. The real filter has a cutoff frequency (F_c) that is less than the Nyquist rate, $F_s/2$. The stop-band aliases $F_a = F_s \pm F_{gen}$ and sample clock are also shown. The intersection of the filter curve with that of the stop-band alias determines the degree of attenuation of the alias component.

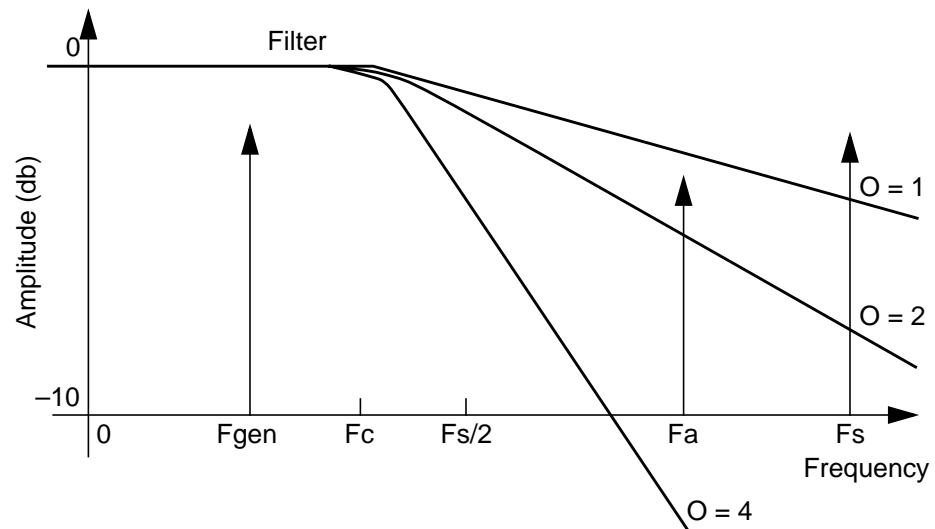


Figure 3. Example Signal and Real Filter Response
O = Order of Filter (1st, 2nd, and 4th Shown)

Filters for signal reconstruction have three important design rules:

1. The passband response should be reasonably flat.
2. The filter cutoff must be somewhat less than the Nyquist rate, but greater than $F_{gen(max)}$.
3. The required filter order is determined by the separation between $F_{gen(max)}$ and $F_s - F_{gen(max)}$.

The flat passband requirement is dictated by the application. Most applications require that signal amplitudes only vary by a small amount across the passband. Typically, Butterworth response is preferred as it has essentially no amplitude ripple in its passband. If the cutoff frequency is chosen too far inside the desired passband (for example, to increase the stop-band attenuation), amplitude distortion (known as twist) can also result which can disrupt the function of tone receivers or detectors (particularly important for dual tone systems).

Once the cutoff frequency is chosen so as to minimize the pass-band distortion, the filter order (for example, the slope of the stop-band attenuation) can be determined by the amount of stop-band alias attenuation required and the system parameters. Better than 40db

attenuation in the stop-band is generally a safe figure, although more or less attenuation may be appropriate for a particular system design.

Each order of filtering results in an attenuation slope of approximately 6db/octave in the filter stop-band. Given filter cutoff, F_c , and a target frequency, F , the following equation relates F_c and F in terms of octaves:

$$(7) \quad F_c * 2^x = F, \text{ or}$$

$$2^x = F/F_c$$

where x = number of octaves of separation.

To solve for x , the log function is used:

$$(8) \quad x = \log (F / F_c) / \log(2)$$

For a given filter order, O , and cut-off frequency, F_c , the attenuation at a particular frequency, $A(F)$, can be calculated from this formula:

$$(9) \quad A(F) = (O * 6\text{db} / \text{octave}) * x \text{ octaves}$$

$$= (6 \text{ db} * O) * (\log (F / F_c) / \log(2))$$

Which can be quickly re-arranged to solve for O :

$$(10) \quad O = A(F) * \log(2) / (6 \text{ db} * \log (F / F_c))$$

O is a unitless quantity and is rounded to the nearest integer.

If the user assumes that the alias and F_s components are approximately equal to the amplitude of the fundamental signal (This is generally true \pm a few db for PWM and DAC systems.), $A(F)$ can be taken as the absolute desired attenuation floor and equation 10 can be used to determine the required filter order based on the fundamental stop-band alias, $F_s - F_{gen(max)}$ (which is typically the most important component to eliminate).

Simple RC stages can be used for applications where order is calculated at 2 or less. However, higher order filters usually require an active design (such as switched capacitor or op-amp based filters) to reduce the pass-band attenuation inherent in passive RC filters.

For most of the firmware examples presented here, these parameters were used:

$$F_s = 7.812 \text{ kHz}$$

$$F_{gmax} = 2.6 \text{ kHz}$$

$$F_c = 3 \text{ kHz}$$

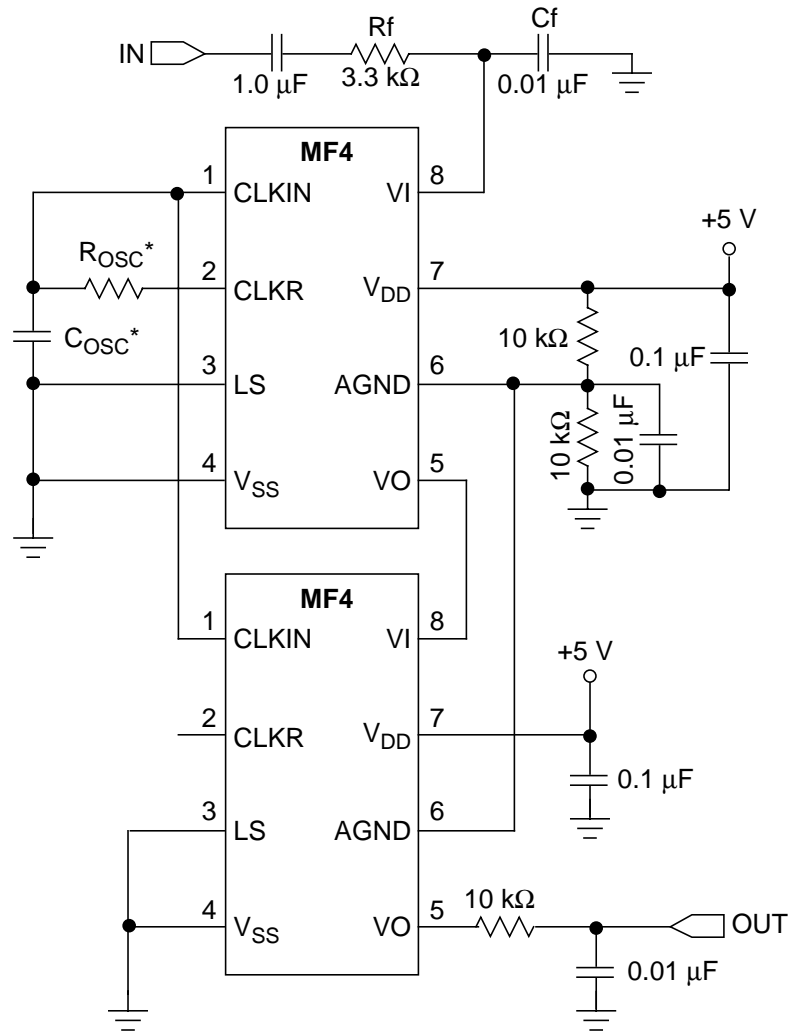
$$A(F_{mas}) = 40 \text{ db}$$

from equation 10,

$$\begin{aligned} O &= A(F_{max}) * \log(2) / (6 \text{ db} * \log((F_s - F_{gmax}) / F_c)) \\ &= 40 \text{ db} * \log(2) / (6 \text{ db} * \log [(7812 - 2600) / 3000]) \\ &= 8.36 \end{aligned}$$

Thus, an eighth order filter would ensure that the stop-band aliases would be better than 40 db below the fundamental. The most effective filter method for higher order designs is a switched capacitor filter such as the MF-4. These devices allow relatively high filter orders with few parts.

The schematic of **Figure 4** shows an eighth order filter with RC input and output filters (needed to remove high frequency noise) for a total filter order of 10, or about 60db/octave. This is the reconstruction filter used with the all of the following examples.



* R_{OSC} and C_{OSC} set F_c

Figure 4. Example Filter Based on the MF-4 Switched Capacitor Building Clock

One of the results of equation 10 (with respect to the primary stop-band alias, $F_s - F_{gen}$) is that the filter order can be reduced by increasing F_s .

If F_s from the previous example is increased to 31.2 kHz:

$$\begin{aligned}
 F_s &= 31.2 \text{ kHz} \\
 F_{gmax} &= 2.6 \text{ kHz} \\
 F_c &= 3 \text{ kHz} \\
 A(F_{max}) &= 40 \text{ db} \\
 O &= A(F_{max}) * \log(2) / (6 \text{ db} * \log((F_s - F_{gmax}) / F_c)) \\
 &= 40 \text{ db} * \log(2) / (6 \text{ db} * \log((31200 - 2600) / 3000)) \\
 &= 2.05
 \end{aligned}$$

Thus, by simply increasing the sample rate by a factor of 4, the two MF-4s in the example filter can be eliminated. This greatly reduces the filter cost.

Sine Table

Each of the following examples uses a unique sine table. While some effort was made to keep the examples consistent, subtle variations from one MCU implementation to the next can impact the data contained in the sine table. Most of this variation is due to PWM latencies in some of the implementations. The D/A code used also can have a drastic impact on the composition of the sine table (a codec versus a linear D/A, for example).

In general, all of the examples presented here follow the same basic format: The sine table varies between a min and max binary value with a mid-point (or 0) reference that lies at:

$$D/A(0) = \text{min} + ((\text{max} - \text{min}) / 2)$$

Thus, all of the tones generated will have a DC offset. Since min and max typically are close to 0 and 255, respectively, the 0 reference will generally be close to $D/A(255) / 2$.

Since buffered PWM and direct D/A systems generally don't exhibit latency problems, the examples here use a sine table that varies from 1 to 255 (or 0 to 254 for the HC12 PWM) with the 0 reference at 128.

However, unbuffered PWM systems can have min/max values that are not so straightforward and require a different sine table. The C program in [Sine Table Generator C Program](#) illustrates a simple method of generating a generic sine table given minimum, maximum, and number of entries and formats it for assembly as an include file.

Tone Generator Algorithm

Each of the D/A examples to follow are shaped by the subtleties of the particular MCUs chosen for this application note. However, the central tone generator algorithm is substantially similar in all cases. Some MCUs require more memory and/or execution time to code and execute, but they all perform the same tasks in the same fashion to generate the sine wave signal. [Figure 5](#) illustrates the flowchart for this algorithm which is the basis for all of the following examples.

The flow chart has two basic variations. [Figure 5A](#) is for non-buffered systems and uses a temporary holding register for the D/A value. The previously calculated D/A is loaded from the temporary register at the start of the interrupt and immediately transferred to the PWM duty cycle register.

In [Figure 5B](#), for buffered systems, this value can be stored as soon as it is calculated.

HC05 Family

Two different PWM modules are available in the HC05 Family. The HC05B16, HC05B32, and HC05X32 variants have a simple PLM module that can provide an 8-bit PWM output at one of two rates, fast and slow.

At maximum MCU clock rates, the fast mode allows only a 1.95-kHz PWM rate, which limits the utility of tone synthesis since the maximum allowed tone frequency would be only $F_s / 2 = 975$ Hz. Still, this might prove useful in several applications, especially in the generation of CTCSS tones. (The highest CTCSS tone is approximately 250 Hz.)

Another HC05 variant, the MC4, has a more flexible PWM module which can generate buffered PWM at rates of up to about 24 kHz and is buffered.

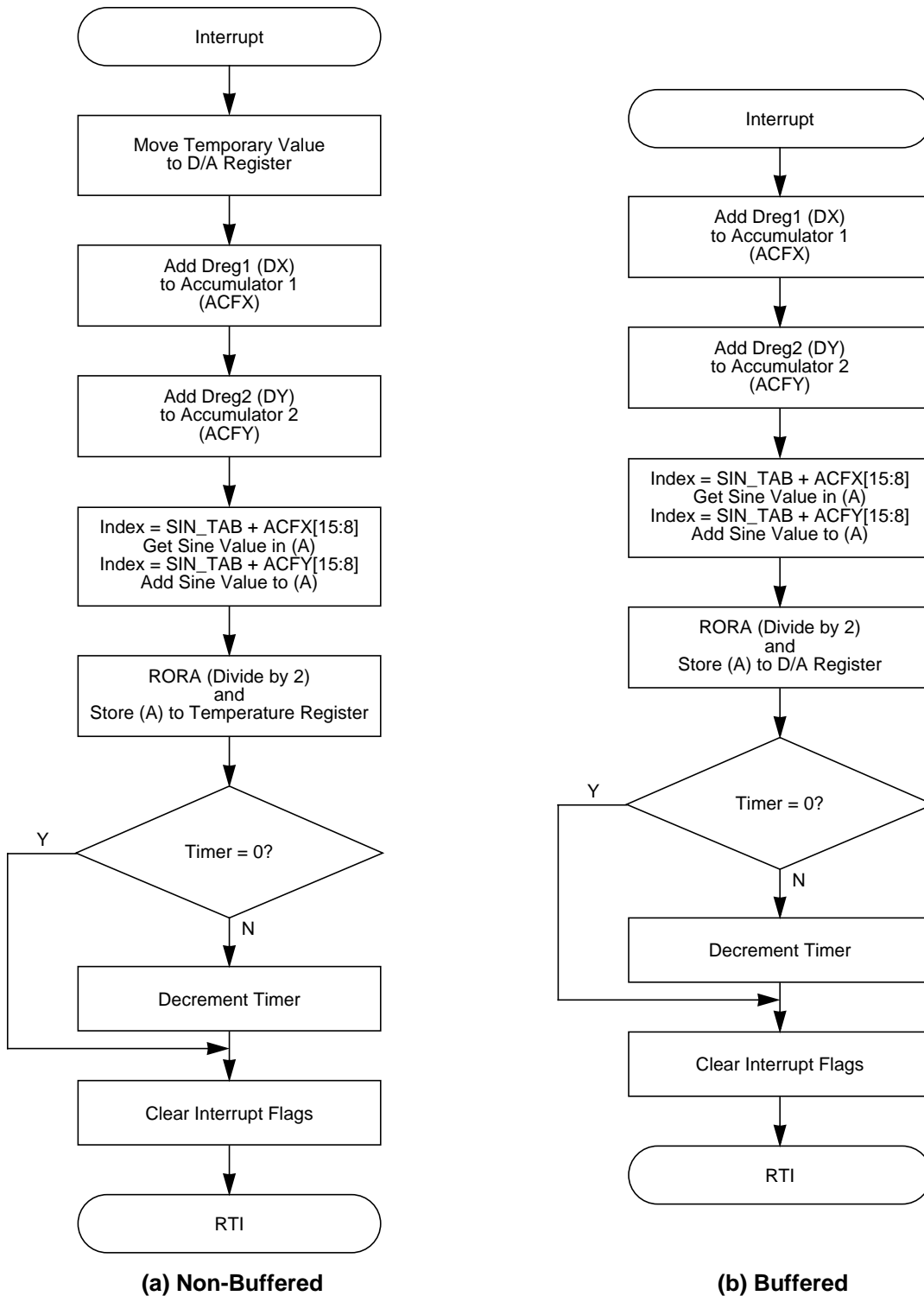


Figure 5. Tone Generator Interrupt Service Flowchart

HC05 PLM

Since the PLM system is not buffered, a crude yet effective technique is used to provide a synchronous interrupt to service the tone generator algorithm. The PWM output is simply connected to one of the input captures which is then configured for falling edge operation. This configuration is effective, but care must be taken to ensure that the PWM avoid 0 percent and 100 percent duty cycles. The PLM does not allow a 100 percent duty cycle, but 0 percent is achievable and must be avoided. If 0 percent is generated by the PLM, the output is a steady logic 0, which effectively disables the tone interrupt. The easiest method to address this situation is to code the sine table so that the min value is at least 1.

NOTE: *It should be noted that, due to interrupt latency, the full 8-bit dynamic range of the PLM is not available.*

The amount of degradation is determined by the interrupt latency, and the amount of time it takes for the interrupt routine to write a new D/A value to the PWM duty cycle register. Because of this requirement, the flowchart of [Figure 5A](#) is used for this example. Since the PLM rate is so low, the MCU latency does not significantly impact the sine table min value. The interrupt latency is 10 cycles, plus a maximum instruction latency of 11 cycles, plus seven cycles of transfer latency equals 28 cycles of latency. However, at a 1.95-kHz PLM rate, it takes four MCU cycles for every PLM counter tick, so the minimum PLM duty cycle is $\text{latency} / 4 = 7$.

HC05MC4 PWM

The MC4 implementation is similar to that of the PLM version in that an input capture is used to source the tone generator interrupt service routine. The MC4 PWM setup is somewhat more complicated in that it offers several features that are targeted at motor applications. For this application, however, we simply want a buffered PWM at a single port pin, which is easily configured as shown in [MC4 PWM](#). Since the PWM is buffered, the D2A temp register that was used in the PLM version can be eliminated and the new D/A value can be written directly to the duty cycle register (PWMAD).

HC08 Buffered PWM

The HC08 PWM module offers a buffered mode by linking two PWM duty cycle registers. Application firmware must track which register was last written to maintain the buffered operation, but this is easily accomplished with a simple counter which is incremented each time a duty cycle register is written. Bit 0 of this counter is used to select which duty cycle register is to be written during any particular interrupt cycle. Since the HC08 PWM uses timer overflow to operate its PWM, it serves as the obvious choice to source the interrupt which drives the tone generator service routine.

HC11 Synchronous PWM

While there are HC11 variants with PWM modules, this example uses two output compares to generate the PWM signal and is thus applicable to all HC11 variants. It is synchronous because the update operation is integrated into the OC interrupt which forces the update to be synchronized with the start of the PWM cycle. However, since the operation is not buffered, dynamic range is affected by response latency (Figure 5A applies).

On the HC11, only one output compare, OC1, can affect any of the OC port pins. All other output compares are tied to a dedicated pin so that the selection of the second OC is tied to a port pin selection and vice versa. For this example, OC1 generates the main interrupt and sets the PWM port pin (PA6) while OC2 clears the port pin.

As illustrated in Figure 6, the OC1 interrupt routine sets both the OC2 and OC1 time-outs and updates the D/A value to be used for the next cycle.

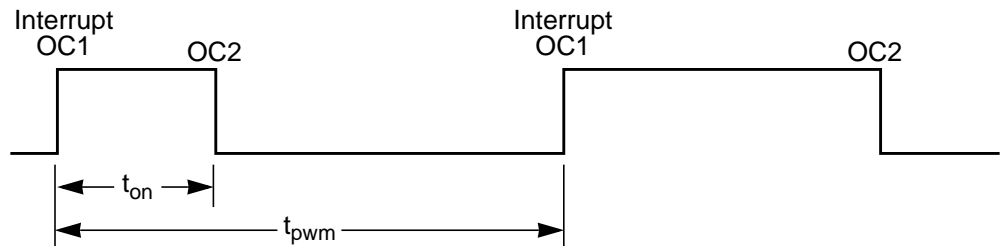


Figure 6. OC1 and OC2 PWM Timings

As indicated in [HC11 PWM Listing](#), the OC1 interrupt requires 29 MCU cycles to stack the registers and update the OC2 timer, which dictates the minimum pulse width. Proper use of the WAI instruction (which pre-stacks the registers on the HC11) can save up to 11 cycles. (WAI takes 14 cycles: 11 cycles to stack registers, plus 3 cycles to fetch the interrupt vector.) Since the vector fetch comes after the interrupt, it gets counted as latency in this example, which reduces the minimum pulse width to $29 - 11 = 18$ cycles. The only restriction on the high end of duty cycle is that the OC2 time-out be less than (for instance, occur prior to) the OC1 time-out value.

NOTE: *The interrupt latency does not account for the instruction that is executing at the time of the interrupt.*

For applications where WAI can not be used or guaranteed, the wide variation in instruction cycles can make the latency calculation a difficult task. Worst case instruction latency would add an additional 41 cycles (IDIV and FDIV) but this can be an excessive step as these instructions are not encountered often in real applications. If the IDIV and FDIV instructions are not used, the figure can be reduced to 10 cycles which will cover all of the remaining instructions while only adding a moderate degree of overhead to the PWM duty cycle.

The following equations determine the critical design constants:

$$\begin{aligned} \text{TSAMP} &= \text{PWM cycle time (cycles)} \\ &= (\text{XTAL} / 4) / \text{Fsamp} \\ &= E / \text{Fsamp} \end{aligned}$$

$$\begin{aligned} \text{TMIN} &= \text{minimum pulse width (cycles)} \\ &= \text{Tint_resp} + \text{Tinstr} + \text{Toc2_update} + 1 \\ &= 14 + 10 + 15 + 1 = 40 \text{ (no WAI)} \\ &= 3 + 0 + 15 + 1 = 19 \text{ (guaranteed WAI)} \end{aligned}$$

$$\begin{aligned} \text{TMAX} &= \text{maximum pulse width (cycles)} \\ &= \text{TSAMP} - 1 \end{aligned}$$

$$\begin{aligned} \text{RANGE} &= \# \text{ discrete steps from min to max} \\ &= \text{TMAX} - \text{TMIN} \end{aligned}$$

$$\begin{aligned} \text{DUTY} &= \text{duty cycle (\%)} \\ &= \text{D2A} / \text{TSAMP} \end{aligned}$$

For this example, a 9.83-MHz crystal was used which gives the following values. The 8-MHz case is also shown.

Table 3. HC11 Design Examples

9.83-MHz Crystal	8-MHz Crystal
$TSAMP = (9.8304E6/4) /$ $7.812 \text{ kHz} = 314 \text{ cycles}$ $TMIN = 40 \text{ cycles (worst case)}$ $TMAX = 313 \text{ cycles}$ $RANGE = 313 - 40$ $= 273$	$TSAMP = (8E6/4) /$ $7.812 \text{ kHz} = 256 \text{ cycles}$ $TMIN = 40 \text{ cycles (worst case)}$ $TMAX = 255 \text{ cycles}$ $RANGE = 255 - 40$ $= 215$

While this example limits the maximum "on" time to eight bits, or 255 timer cycles, the above calculations indicate that greater than eight bits of dynamic range are possible for $E > 2.32 \text{ MHz}$ (for F_{samp} as shown). If maximum dynamic range is of importance and the MCU oscillator design will allow higher crystal frequencies to be selected, the excess RANGE value can be used to absorb the latency figure. This is done by adding the latency into the updated TOC2 value at the end of the OC1 interrupt routine. This method would add nine cycles to the length of the interrupt routine, but would allow a full 8-bit D/A implementation. In this case, the sine table could be calculated to swing from 1 to 255.

HC12 Buffered PWM

For this example (see [HC12 PWM Listing](#)), the HC12 PWM is operated in 8-bit buffered mode. The original design used an output compare interrupt to update the PWM where the OC period was an integer multiple of the PWM period. However, this design exhibited noise problems at high values of PWDT0 and the system was re-worked to follow the HC05 PLM case where the PWM drives an input capture. (PP0 is connected to TC7 as a falling edge triggered interrupt.) For the HC12 PWM module, the duty cycle ranges from 1 / 256 to 256 / 256 for values of PWDT0 that range from 0 to 255. Since the input capture system cannot tolerate duty cycles of 0 percent or 100 percent, these values must be eliminated from the sine table, thus the HC12 PWM sine table should range from 0 to 254 for proper operation.

One difference worthy of note in the HC12 allows the reduction in the length of the sine table. In systems where memory must be conserved,

the addition of the linear interpolate instruction, TBL, can greatly reduce the size of the 256-byte sine table of the previous examples without seriously impacting signal quality. A reduction in N by a factor of 4 or 8 (64- or 32-byte sine length) can be achieved by using the fractional portion of the phase accumulators to supply the interpolation operator used by the TBL instruction. This is a direct extension of the indexing principal defined for the phase accumulators. If the integer portion of the accumulator determines the position in the sine table, the fractional portion determines the fractional phase distance to the next entry.

To keep the system parameters the same as the 256-byte case (same Fstep, Fsamp, Fgen, etc.), the decimal radix for Dreg and the phase accumulators are moved up rather than reducing the range of the integer portion. Since the interpolate operation has the effect of "filling in" the "missing" table entries, the position of the radix is chosen to yield an effective table length of 256 (which simply allows the same Dreg values to be used).

This is accomplished by moving the radix in proportion to the factor of reduction in table length. If the table is divided by a factor of 2^x , then the radix is moved up "x" bits. The example in [Interpolated Table Lookup](#) uses a 32-byte table, which is a factor of 2^3 reduction, thus moving the radix to lie between bits 10 and 11. Shift instructions are used to byte align the radix when extracting the table index and interpolate values.

Direct D/A

A direct D/A interface is a worthwhile alternative to PWM methods in those situations where PWM is not suitable and the additional cost is justified. (See [HC12 DAC Listing](#).) Signal-to-noise improvements can be achieved over most PWM methods, and system clock frequencies can be reduced in some cases to reduce power consumption. There are several well documented methods that can be employed for direct D/A; for this reason, the discussion here focuses on the importance of timing in writing the D/A value to the D/A sub-system.

As mentioned earlier regarding PWM systems, buffered operation is preferred over non-buffered due to the way in which changes in the duty

cycle (for instance, new D/A values) are synchronized to the sample clock. This is also important in direct D/A sub-systems because a statistical variation of even a single CPU clock cycle can result in significant noise in the output. For interrupt-driven systems, instruction latencies introduced in the interrupt dispatch can easily account for several CPU cycles of variation in the timing of the D/A update. A simple mechanism for precisely controlling the D/A update is needed.

The simplest approach is to use the WAI (or WAIT, depending on the processor source form) instruction to ensure that the CPU has been configured in anticipation of the coming interrupt. Once the wait instruction is complete, the subsequent interrupt response latency will be consistent for each iteration of the interrupt.

This approach has two basic difficulties:

1. The designer must make sure that a wait instruction is executed prior to each and every interrupt. While this is relatively straightforward for simple systems, it may not be feasible to maintain for more complicated systems, especially if interrupt recursion is used.
2. Other interrupt sources may disrupt the D/A update process which dictates, in general, that other interrupts must be disabled during tone generation.

Another approach requires the addition of a latch and the use of an output compare signal to latch the new value into the D/A after the interrupt firmware has written the D/A update. The output compare will then be synchronized to the CPU clock with no excessive firmware maintenance issues. As long as the tone generator interrupt can be adequately serviced, the D/A latch can be precisely synchronized to the CPU clock. The external latch approach also allows I/O (input/output) expansion to reclaim the bits used to drive the D/A for other I/O functions.

This method is illustrated in **Figure 7**. The DAC0832 is designed to interface to a processor bus and features a built-in double-buffered latch. One interface signal (\sim WR) latches the initial write, while another interface signal (\sim XFER) transfers the latched data to the D/A.

An output compare signal drives the \sim XFER signal which assures that the data is always presented to the D/A at the exact sample point relative to the previous sample period.

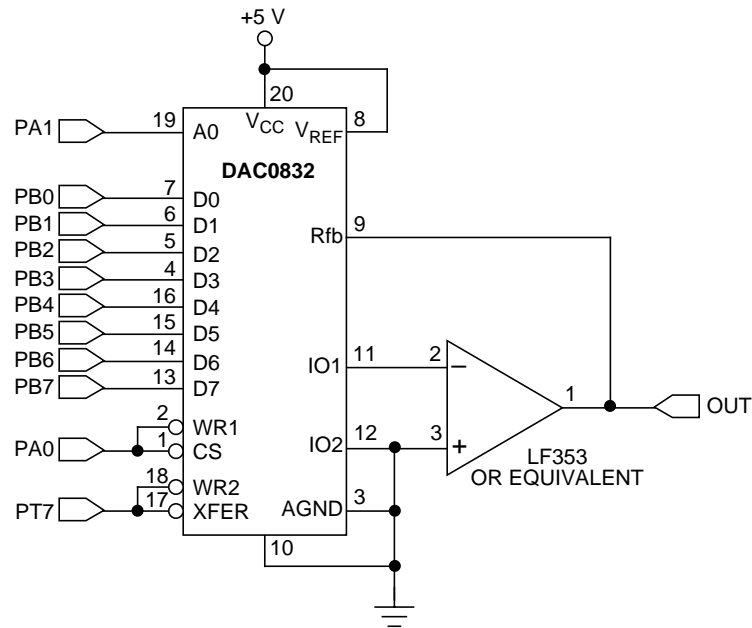


Figure 7. DAC MCU Connections

The output compare also serves as the tone generator interrupt source as it occurs at the sample rate. Once the interrupt is processed, the code clears the XFER signal and updates the phase accumulators. The updated values are then used to calculate the new D/A value which is then written to the D/A port which arms the D/A transfer mechanism. When the next output compare is issued, the D/A will transfer the value previously written and repeat the procedure.

Freescale Semiconductor, Inc.

DTMF and Call-Progress Tones

TELCO and wireless applications are two areas which make wide use of DTMF and call-progress signaling. Both DTMF and call-progress signaling systems make use of dual tones to signify a unique system state.

Tone Definitions

Table 4 lists the tone formats for the various signaling states.

Table 4. TDMF and Call Progress Frequency List

State Description	High Tone	Low Tone (Hz)	Fs = 7.812 kHz	
			High Tone Dreg (Decimal)	Low Tone Dreg (Decimal)
Dial tone	440 ± 5%	350 ± 0.5%	3691	2936
Busy *	620 ± 5%	480 ± 0.5%	5201	4026
Ringback *	480 ± 5%	440 ± 0.5%	4026	3691
Note: All DTMFs ± 0.5%				
DTMF "1"	1209 ± 5%	697 ± 5%	10142	5847
DTMF "2"	1336	697	11207	5847
DTMF "3"	1477	697	12316	5847
DTMF "4"	1209	770	10142	6459
DTMF "5"	1336	770	11207	6459
DTMF "6"	1477	770	12316	6459
DTMF "7"	1209	852	10142	7147
DTMF "8"	1336	852	11207	7147
DTMF "9"	1477	852	12316	7147
DTMF "0"	1336	941	11207	7894
DTMF "**"	1209	941	10142	7894
DTMF "#"	1477	941	12316	7894
DTMF "A"	1633	697	13698	5847
DTMF "B"	1633	770	13698	6459
DTMF "C"	1633	852	13698	7147
DTMF "D"	1633	941	13698	7894

* Busy tone cycles on/off at 0.5 s/0.5s, ringback tone cycles on/off at 2 s / 4 s.

To calculate the absolute frequency tolerance one must take the lowest frequency in the table, 350 Hz, and apply equation 6:

$$\begin{aligned}
 F_{\text{step(max)}} &= F_{\text{min}} * \% \text{error} \\
 &= 350 * 0.005 \\
 &= 1.75 \text{ Hz}
 \end{aligned}$$

All of the examples presented here meet this Fstep specification with no difficulty (although the HC05 PWM example would not be able to generate the DTMF tones due to its limitation on Fs).

	1209 Hz	1336 Hz	1477 Hz	1633 Hz
697 Hz	1	2	3	A
770 Hz	4	5	6	B
752 Hz	7	8	9	C
941 Hz	*	0	#	D

Figure 8. Standard DTMF Keypad Layout and Frequency Matrix

Due to the legacy of the original Bell Telephone DTMF keypad layout, it is still common to depict the DTMF row/column format as shown in **Figure 8**. This layout is helpful in that the intersecting rows and columns correspond to the frequencies of each signal. A binary "2 of 8" code is often used to represent DTMF digits as the row and column frequencies can be easily extracted. In the 2 of 8 code, four bits are used to represent the 16 DTMF signals. The upper two bits specify the row frequency,

while the lower two bits specify the column frequency as illustrated in [Table 3](#).

Table 5. ASCII to 2 of 8 Conversion Matrix

2 of 8	ASCII
0000	1
0001	2
0010	3
0011	A
0100	4
0101	5
0110	6
0111	B
1000	7
1001	8
1010	9
1011	C
1100	*
1101	0
1110	#
1111	D

Sample TELCO Routines

TELCO Subroutines shows the HC11/HC12 routines that are used to demonstrate the DTMF and call-progress tones. The main subroutine is DTMFstr which takes an EOL (\$0D) terminated ASCII string and converts it to the DTMF equivalents for each tone using ASCdtmf. The constants "toneon" and "toneoff" specify the on and off timings for the DTMF signals and are shown at their typical values in this listing (40 ms on/off).

ASCdtmf converts the ASCII character in (A) to a 2 of 8 code using the ordered ASC_T look-up table. The 2 of 8 code is then used to access the DTMFlo and DTMFhi look-up tables to extract the desired Dreg values which are copied to the DX and DY registers. Lastly, the ASCdtmf uses the tontimer to time the on and off portions of the tone before exiting.

Since most of the MCU execution time is spent waiting for tontimer to count down to 0, these loops can contain a JSR to a system polling subroutine to perform non-critical real-time system functions. As long as the polling routine takes less than $(1 / Fs) - T_{interrupt}$, the system throughput will not be impacted inversely.

The call-progress tones are generated by CPsub. The tone generated is determined by the contents of the (A) register upon entry into the routine. (A) = "D" generates a dial tone, (A) = "B" generates a busy tone, while (A) = "R" generates a ringback tone. All of the call progress tones continue until an SCI character is detected. In a real-world application, an I/O signal and/or timer combination likely would be used to terminate these tones.

Conclusion

The techniques described herein demonstrate the feasibility of implementing a sine-wave-based tone generation system on a variety of Motorola microcontroller families. By using interrupts to synchronize the tone generation algorithm, the system may be integrated easily in to any system without having to re-calibrate machine cycles in timing loops. The interrupt nature of the system also allows for real-time I/O service for application specific functions. This allows a wide variety of tone signaling protocols to be supported easily with a minimum of code and data overhead.

Listings

HC05 PWM Listings

HC05 PLM

Setup:

```

188      ; init pwm (PLMA)
189      ; NOTE: MOR must select /1 clock prescale
190
0401    B60C  191    LDA     MISC
0403    A4F5  192    AND     #$FF^(SFA|SM)      ; set pwm period = fast
0405    B70C  193    STA     MISC              ; = 1.92 kHz @ X = 8 Mhz
0407    A680  194    LDA     #$80              ; preset @50% duty
0409    B70A  195    STA     PLMA
196
197      ; init IC1
198
040B    B612  199    LDA     TCR
040D    AA82  200    ORA     #ICIE|IEDG1
040F    B712  201    STA     TCR
202
0411    9A    203    CLI
    
```

Interrupt service:

```

269      ; icii traps PLM edges to synch the PWM update
270      ; fsamp rate is determined by PLM period ...
271      ; new SIN_TAB pointers are calculated for next
272      ; sample period. D2A is < 8 bits due to
273      ; response latency of IC interrupt.
274
0430    B65A  275    icii  LDA     D2A
0432    B70A  276    STA     PLMA              ; update PLM
0434    B613  277    LDA     TSR              ; clear interrupt flags
0436    B615  278    LDA     TIC1L
0438    B61D  279    LDA     TIC2L
043A    B651  280    LDA     DX+1              ; do accum for tone 1
043C    BB57  281    ADD     ACFX+1
043E    B757  282    STA     ACFX+1
0440    B650  283    LDA     DX
0442    B956  284    ADC     ACFX
0444    B756  285    STA     ACFX
0446    B653  286    LDA     DY+1              ; do accum for tone 2
0448    BB59  287    ADD     ACFY+1
044A    B759  288    STA     ACFY+1
044C    B652  289    LDA     DY
044E    B958  290    ADC     ACFY
    
```

AN1771

Application Note

```

0450    B758    291    STA     ACFY
0452    BE56    292    LDX     ACFX                ; lookup tone 1
0454    D60474 293    LDA     SIN_TAB,X
0457    BE58    294    LDX     ACFY                ; lookup tone 2
0459    DB0474 295    ADD     SIN_TAB,X
045C    46      296    RORA                    ; div by 2 to get 8 bits
045D    B75A    297    STA     D2A                ; store for next update
045F    B654    298    LDA     tontimer          ; update duration count
0461    2604    299    BNE     loop4             ; done,
0463    B655    300    LDA     tontimer+1
0465    270C    301    BEQ     icix              ; done,
0467    B655    302    loop4   LDA     tontimer+1   ; tontimer--
0469    A001    303    SUB     #$01
046B    B755    304    STA     tontimer+1
046D    B654    305    LDA     tontimer
046F    A200    306    SBC     #$00
0471    B754    307    STA     tontimer
0473    80      308    icix   RTI
    
```

MC4 PWM

Setup:

```

                28    ; init pwm
                29
0101    A641    30    LDA     #CSA1+POLA        ; enable pwm1
0103    B714    31    STA     CTLA
0105    A690    32    LDA     #9*10           ; set 7.8 kHz pwm rate
0107    B716    33    STA     RATE
0109    A680    34    LDA     #$80           ; preset D/A @ zero
010B    B710    35    STA     PWMAD
                36
                37    ; init IC1
                38
010D    A682    39    LDA     #ICIE2|IEDG2    ; ic2 on, rising edge
0111    B717    40    STA     TCR
    
```

Interrupt service:

```

                110    ; iclii traps PLM edges to synch the PWM update
                111    ; fsamp rate is determined by PWM period ... new
                112    ; SIN_TAB pointers are calculated for next
                113    ; sample period.
                114
0132    B618    115    iclii   LDA     TSR                ; clear int flags
0134    B61C    116    LDA     TIC1L
0136    B61A    117    LDA     TIC2L
0138    B651    118    LDA     DX+1                ; do accum for tone 1
013A    BB57    119    ADD     ACFX+1
013C    B757    120    STA     ACFX+1
013E    B650    121    LDA     DX
0140    B956    122    ADC     ACFX
    
```



```

0142    B756    123    STA    ACFX
0144    B653    124    LDA    DY+1                ; do accum for tone 2
0146    BB59    125    ADD    ACFY+1
0148    B759    126    STA    ACFY+1
014A    B652    127    LDA    DY
014C    B958    128    ADC    ACFY
014E    B758    129    STA    ACFY
0150    BE56    130    LDX    ACFX                ; lookup tone 1
0152    D60172  131    LDA    SIN_TAB,X
0155    BE58    132    LDX    ACFY                ; lookup tone 2
0157    DB0172  133    ADD    SIN_TAB,X
015A    46      134    RORA                   ; div by 2 to get 8 bits
015B    B710    135    STA    PWMAD            ; store to d/a
015D    B654    136    LDA    tontimer        ; update duration count
015F    2604    137    BNE    loop4           ; done,
0161    B655    138    LDA    tontimer+1
0163    270C    139    BEQ    icix           ; done
0165    B655    140    loop4    LDA    tontimer+1    ; tontimer--
0167    A001    141    SUB    #$01
0169    B755    142    STA    tontimer+1
016B    B654    143    LDA    tontimer
016D    A200    144    SBC    #$00
016F    B754    145    STA    tontimer
0171    80      146    icix    RTI

```

Application Note

HC08 PWM Listing

Setup:

```

489          ; init pwm
490
6E07    B620    491    LDA     TSC                ; stop timer
6E09    AA30    492    ORA     #TSTOP|TRST
6E0B    B720    493    STA     TSC
6E0D    4500FF 494    LDHX   #pwper                ; set pwm period
6E10    3524    495    STHX   TMOD
6E12    450080 496    LDHX   #$0080                ; init duty cycle
6E15    3527    497    STHX   TCH0
6E17    A601    498    LDA     #1                    ; init tracking register
6E19    B75A    499    STA     track
6E1B    A62A    500    LDA     #MS0B|TOV0|ELS0B
6E1D    B726    501    STA     TSC0                ; init ch1 = buffered
6E1F    B620    502    LDA     TSC                ; stop timer
6E21    A4DF    503    AND     #$FF^TSTOP
6E23    AA40    504    ORA     #TOIE
6E25    B720    505    STA     TSC
6E27    9A     506    CLI

```

Interrupt service:

```

562          ; tovi sets the fsamp rate and calculates new
563          ; SIN_TAB pointers for next sample period. D2A
564          ; is 8 bits only!
565
6E44    B620    566    tovi  LDA     TSC                ; clear int flag
6E46    A47F    567    AND     #$FF^TOF
6E48    B720    568    STA     TSC
6E4A    B651    569    LDA     DX+1                ; do accum for tone 1
6E4C    BB57    570    ADD     ACFX+1
6E4E    B757    571    STA     ACFX+1
6E50    B650    572    LDA     DX
6E52    B956    573    ADC     ACFX
6E54    B756    574    STA     ACFX
6E56    B653    575    LDA     DY+1                ; do accum for tone 2
6E58    BB59    576    ADD     ACFY+1
6E5A    B759    577    STA     ACFY+1
6E5C    B652    578    LDA     DY
6E5E    B958    579    ADC     ACFY
6E60    B758    580    STA     ACFY
6E62    8C     581    CLRH
6E63    BE56    582    LDH   ACFX                ; lookup tone 1
6E65    D66E84 583    LDA     SIN_TAB,X
6E68    8C     584    CLRH
6E69    BE58    585    LDH   ACFY                ; lookup tone 2
6E6B    DB6E84 586    ADD     SIN_TAB,X
6E6E    46     587    RORA                ; div by 2 to get 8 bits
6E6F    450028 588    LDHX   #TCH0L                ; test which pwm to write
6E72    015A03 589    BRCLR  0,track,loop3        ; is ch0,
6E75    45002B 590    LDHX   #TCH1L                ; switch to ch1
6E78    F7     591    loop3 STA     ,X                ; set for next cycle
6E79    3C5A    592    INC     track                ; update tracking reg
6E7B    5554    593    LDHX   tontimer            ; update duration count
6E7D    2704    594    BEQ     loop4                ; done,
6E7F    AFFF    595    AIX     #-1t                ; x--
6E81    3554    596    STHX   tontimer
6E83    80     597    loop4 RTI

```

HC11 PWM Listing

Setup:

```

443          ; TON enables oc1 tone generator
444
445      8064      8640TONLDAA      #OC1M6          ; oc1 sets PA6
446      8066      B7100C STAA      OC1M
447      8069      8640      LDAA      #OC1D6
448      806B      B7100D STAA      OC1D
449      806E      B61020 LDAA      TCTL1          ; oc2 clears PA6
450      8071      843F      ANDA      #~(OM2|OL2)
451      8073      8A80      ORAA      #OM2
452      8075      B71020 STAA      TCTL1
453      8078      FC100E LDD      TCNT          ; init oc1 rate
454      807B      C30133 ADDD      #TSAMP
455      807E      FD1016 STD      TOC1
456      8081      961E      LDAA      TMIN          ; init d2a
457      8083      9708      STAA      D2A
458      8085      FC100E LDD      TCNT          ; preset OC2 near bottom
459      8088      D31E      ADDD      TMIN
460      808A      D31E      ADDD      TMIN
461      808C      FD1018 STD      TOC2
462      808F      86C0      LDAA      #OC1F|OC2F      ; pre-clear oc flags
463      8091      B71023 STAA      TFLG1
464      8094      B61022 LDAA      TMSK1          ; enable oc1 interrupt
465      8097      8A80      ORAA      #OC1F
466      8099      B71022 STAA      TMSK1
467      809C      39          RTS
468          ;
469          ;
470          ; TOFF disables oc1 tone generator
471
472      809D      B61022 TOFF      LDAA TMSK1          ; disable oc1 interrupt
473      80A0      847F      ANDA      #~OC1F
474      80A2      B71022 STAA      TMSK1
475      80A5      7F100C CLR      OC1M          ; disconnect timer pins
476      80A8      B61020 LDAA      TCTL1
477      80AB      843F      ANDA      #~(OM2|OL2)
478      80AD      B71020 STAA      TCTL1
479      80B0      39          RTS
    
```

Application Note

Interrupt service:

```

482                ; OC1III handles oc1 interrupts by setting fsamp
483                ; pace and calculating new SIN_TAB pointers for
484                ; next sample period. D2A is 8bits only! Cycle
485                ; times assume DIR addressing for non-MCU
486                ; locs, & EXT addressing for all other locs.
487
488                ;~14 for interrupt
489    80B1    DC08    OC1I    LDD    D2A    ;~4 get pwm from last d/a
490    80B3    F31016  ADDD    TOC1    ;~6
491    80B6    FD1018  STD     TOC2    ;~5
492                ;  ~= ~14 + ~15 = ~29
493
494    80B9    FC1016  LDD     TOC1    ;~5 set pwm rate
495    80BC    C30133  ADDD    #TSAMP   ;~4
496    80BF    FD1016  STD     TOC1    ;~5
497    80C2    DC00    LDD     DX      ;~4 do accum for tone 1
498    80C4    D304    ADDD    ACFX    ;~5
499    80C6    DD04    STD     ACFX    ;~4
500    80C8    DC02    LDD     DY      ;~4 do accum for tone 2
501    80CA    D306    ADDD    ACFY    ;~5
502    80CC    DD06    STD     ACFY    ;~4
503    80CE    CE80F3  LDX     #SIN_TAB ;~3 lookup tone 1
504    80D1    D604    LDAB   ACFX    ;~3
505    80D3    3A     ABX     ;~3
506    80D4    A600    LDAA   0,X     ;~4
507    80D6    CE80F3  LDX     #SIN_TAB ;~3 lookup tone 2
508    80D9    D606    LDAB   ACFY    ;~3
509    80DB    3A     ABX     ;~3
510    80DC    AB00    ADDA   0,X     ;~4 add to 1st tone
511    80DE    46     RORA    ;~2 div by 2 to get 8 bits
512
513                IF     BIT8     ; slower method (8 bit d/a)
514    80DF    16     TAB     ;~2
515    80E0    4F     CLRA    ;~2
516    80E1    C3001E  ADDD    #TMIN   ;~4 add TMIN to d/a
517    80E4    DD08    STD     D2A     ;~4 save for next sample
518
519                ELSE    ; quick method( < 8 bit d/a)
520                ENDIF
521
522    80E6    DE0A    LDX     tontimer ;~5 update tone duration
523    80E8    2703    BEQ     :03     ;~3 done,
524    80EA    09     DEX     ;~3
525    80EB    DF0A    STX     tontimer ;~5
526    80ED    86C0:03 LDAA   #OC1F|OC2F ;~2
527    80EF    B71023  STAA   TFLG1    ;~4
528    80F2    3B     RTI     ;~12
529                ;  == 134 (BIT8 = false)
530                ;  == 143 (BIT8 = true)

```

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HC12 PWM Listing

Setup:

```

1034                                     ; timer inits
1035
1036      0820      8600      LDAA      #0                                     ; TC7 = IC
1037      0822      5A80      STAA      TIOS
1038      0824      8680      LDAA      #EDG7B                               ; falling edge
1039      0826      5A8A      STAA      TCTL3
1040      0828      8680      LDAA      #TEN                                 ; enable timer
1041      082A      5A86      STAA      TSCR
1042      082C      8608      LDAA      #TCRE
1043      082E      5A8D      STAA      TMSK2
1044      0830      8680      LDAA      #C7I
1045      0832      5A8C      STAA      TMSK1
1046      0834      CC0871  LDD      #tc7ii                                 ; init the interrupt vector
1047      0837      7C0B20  STD      tc7vec
1048
1049                                     ; init pwm channel 0
1050
1051      083A      8600      LDAA      #0                                     ; 32 kHz sample rate ;PCKA1
1052      083C      5A40      STAA      PWCLK                               ; separate PWMs, /1 prescale
1053      083E      790041  CLR      PWPOL                               ; clock A for PWM0
1054      0841      790054  CLR      PWCTL                               ;non-center,PWM runs in wait
1055      0844      86FF      LDAA      #255
1056      0846      5A4C      STAA      PWPER0                             ; set pulse period
1057                                     ; = (chA period) * (255 + 1)
1058                                     ; = 1/E * 256
1059                                     ; = 32 μS (31.25 kHz) @ E = 8 MHz
1060                                     ; this is exactly 4x Fsamp
1061      0848      8601      LDAA      #PWEN0                             ; enable PWM0
1062      084A      5A42      STAA      PWEN
1063      084C      CC0000  LDD      #0
1064      084F      8680      LDAA      #$80
1065      0851      5A50      STAA      PWDTY0                             ; init d/a register
1066
1067      0853      10EF      CLI

```

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MOTOROLA

For More Information On This Product,
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Application Note

Normal Table Lookup

Interrupt service:

```

1113             ; tc7ii sets the fsamp rate and calculates new
1114             ; SIN_TAB pointers for next sample period.
1115
1116                                     ;~9 for interrupt
1117 0871 8680 tc7iiLDAA #C7F             ;~1
1118 0873 5A8E STAA TFLG1                 ;~3
1119 0875 FC0800 LDD DX                   ;~3 do accum for tone 1
1120 0878 F30806 ADDD ACFX               ;~3
1121 087B 7C0806 STD ACFX                 ;~2
1122 087E FC0802 LDD DY                   ;~3 do accum for tone 2
1123 0881 F30808 ADDD ACFY               ;~3
1124 0884 7C0808 STD ACFY                 ;~2
1125 0887 CE0D00 LDX #SIN_TAB            ;~2 lookup tone 1
1126 088A F60806 LDAB ACFX               ;~3
1127 088D 1AE5 ABX                       ;~2
1128 088F A600 LDAA 0,X                  ;~3
1129 0891 CE0D00 LDX #SIN_TAB            ;~2 lookup tone 2
1130 0894 F60808 LDAB ACFY               ;~3
1131 0897 1AE5 ABX                       ;~2
1132 0899 AB00 ADDA 0,X                  ;~3 add to 1st tone
1133 089B 46 RORA                        ;~1 div by 2 to get 8 bits
1134 089C 5A50 STAA PWDTY0               ;~3 save to d/a
1135 089E FE0804 LDX tontimer            ;~3 update tone duration?
1136 08A1 2704 BEQ L3                    ;~3 no, done,
1137 08A3 09 DEX                          ;~1 decrement tone timer
1138 08A4 7E0804 STX tontimer            ;~2
1139 08A7 0B L3 RTI                      ;~8
1140                                     ; ~~ = 70

```

Interpolated Table Lookup

Interrupt service:

```

1340             ; tc7ii sets the fsamp rate and calculates new
1341             ; SIN_TAB pointers for next sample period.
1342
1343                                     ;~9 for interrupt
1344 0D4E 8680 tc7ii LDAA #C7F             ;~1
1345 0D50 5A8E STAA TFLG1                 ;~3
1346 0D52 FC0800 LDD DX                   ;~3 do accum for tone 1
1347 0D55 F30806 ADDD ACFX               ;~3
1348 0D58 7C0806 STD ACFX                 ;~2
1349 0D5B FC0802 LDD DY                   ;~3 do accum for tone 2
1350 0D5E F30808 ADDD ACFY               ;~3
1351 0D61 7C0808 STD ACFY                 ;~2

```

```

1352
1353         ; interpolate lookup goes here
1354
1355         ; INCLUDE "LOOKUP.ASM"      ;~20
1356         INCLUDE "INTERP.ASM"      ;~45
1357         ; interpolate table lookup code
1358         ; Adds 25 MCU cycles over standard version
1359         ; uses 32 byte sine table.
1360
1361 0D64 FC0806 LDD      ACFX          ;~3 move radix (tone 1)
1362 0D67 49     LSRD          ;~1
1363 0D68 49     LSRD          ;~1
1364 0D69 49     LSRD          ;~1
1365 0D6A B781  EXG      A,B          ;~1 calculate table address
1366 0D6C CE0D9B LDX      #SIN_TAB     ;~2
1367 0D6F 1AE5  ABX          ;~2
1368 0D71 B781  EXG      A,B          ;~1 B = fractional phase
1369 0D73 183D00 TBL      0,X         ;~8 interpolate
1370 0D76 7A080A STAA     temp        ;~2
1371 0D79 FC0808 LDD      ACFY          ;~3 move radix (tone 2)
1372 0D7C 49     LSRD          ;~1
1373 0D7D 49     LSRD          ;~1
1374 0D7E 49     LSRD          ;~1
1375 0D7F B781  EXG      A,B          ;~1 calculate table address
1376 0D81 CE0D9B LDX      #SIN_TAB     ;~2
1377 0D84 1AE5  ABX          ;~2
1378 0D86 B781  EXG      A,B          ;~1 B = fractional phase
1379 0D88 183D00 TBL      0,X         ;~8 interpolate
1380 0D8B BB080A ADDA     temp        ;~3 add to 1st tone
1381                                     ; ~~ = 45
1382
1383         ; end of lookup, (A) = PWM value
1384
1385 0D8E 46     RORA          ;~1 div by 2 to get 8 bits
1386 0D8F 5A50  STAA     PWDTY0       ;~3 save to d/a
1387 0D91 FE0804 LDX      tontimer     ;~3 update tone duration?
1388 0D94 2704  BEQ      L8           ;~3 no, done,
1389 0D96 09     DEX          ;~1 decrement tone timer
1390 0D97 7E0804 STX      tontimer     ;~2
1391 0D9A 0B L8  RTI          ;~8
1392         ; ~~ = 70 (~95 for interpolate version)
1393         ;

```

Application Note

HC12 DAC Listing

Setup:

```

1038                                     ; timer inits
1039
1040      0820      8680      LDAA      #IOS7
1041      0822      5A80      STAA      TIOS
1042      0824      8680      LDAA      #TEN
1043      0826      5A86      STAA      TSCR
1044      0828      8608      LDAA      #TCRE
1045      082A      5A8D      STAA      TMSK2
1046      082C      8680      LDAA      #OM7
1047      082E      5A88      STAA      TCTL1
1048
1049      0830      8680      LDAA      #C7I
1050      0832      5A8C      STAA      TMSK1
1051      0834      CC0400    LDD      #1024          ; 7.8125 kHz fsamp
1052      0837      5C9E      STD      TC7
1053      0839      CC0870    LDD      #tc7ii
1054      083C      7C0B20    STD      tc7vec
1055
1056                                     ; init DAC port I/O
1057
1058      083F      86FF      LDAA      #$FF
1059      0841      5AAF      STAA      DDRT
1060      0843      86FF      LDAA      #$FF
1061      0845      5A03      STAA      DDRB
1062      0847      86FF      LDAA      #$FF
1063      0849      5A02      STAA      DDRA
1064      084B      8606      LDAA      #$06
1065      084D      5A00      STAA      PORTA
1066      084F      8680      LDAA      #DACXFR
1067      0851      5AAE      STAA      PORTT
1068
1069      0853 10EF      CLI

```


Interrupt service:

```

1113          ; tc7ii sets the fsamp rate and calculates new
1114          ; SIN_TAB pointers for next sample period.
1115          ; D2A is 8 bits only!
1116
1117 086C      8680 tc7iiLDAA    #C7F
1118 086E      5A8E      STAA    TFLG1
1119 0870      86C0      LDAA    #OM7+OL7          ; reset XFER pin to "1"
1120 0872      5A88      STAA    TCTL1
1121 0874      8680      LDAA    #FOC7
1122 0876      5A81      STAA    CFORC
1123 0878      A7        NOP
1124 0879      8680      LDAA    #OM7
1125 087B      5A88      STAA    TCTL1
1126 087D      FC0800    LDD     DX          ; do accum for tone 1
1127 0880      F30806    ADDD    ACFX
1128 0883      7C0806    STD     ACFX
1129 0886      FC0802    LDD     DY          ; do accum for tone 2
1130 0889      F30808    ADDD    ACFY
1131 088C      7C0808    STD     ACFY
1132 088F      CE0D00    LDX     #SIN_TAB      ; lookup tone 1
1133 0892      F60806    LDAB   ACFX
1134 0895      1AE5      ABX
1135 0897      A600      LDAA    0,X
1136 0899      CE0D00    LDX     #SIN_TAB      ; lookup tone 2
1137 089C      F60808    LDAB   ACFY
1138 089F      1AE5      ABX
1139 08A1      AB00      ADDA    0,X
1140 08A3      46        RORA          ; div by 2 to get 8 bits
1141 08A4      5A01      STAA    PORTB      ; write data to port
1142 08A6      84FD      ANDA    #$FD        ; strobe write
1143 08A8      5A00      STAA    PORTA
1144 08AA      A7        NOP
1145 08AB      A7        NOP
1146 08AC      8A02      ORAA    #DACS
1147 08AE      5A00      STAA    PORTA
1148 08B0      FE0804    LDX     tontimer      ; update tone duration
1149 08B3      2704      BEQ     L3          ; done,
1150 08B5      09        DEX
1151 08B6      7E0804    STX     tontimer
1152 08B9      0B L3     RTI

```

Application Note

TELCO Subroutines

```

1036 0F42 halfsec EQU 3906 ; = time * Fsamp
1037 04B0 toneon EQU 1200 ; = time * Fsamp
1038 0258 toneoff EQU 600 ; = time * Fsamp
1039 000D EOL EQU $0D ; end of line
1040 0B78 dialow EQU 2936 ; dial low tone
1041 0E6B dialhi EQU 3691 ; dial high tone
1042 0032 ringcount EQU 50 ; max # ring cycles
1043 0E6B ringlow EQU 3691 ; ring low tone
1044 0FBA ringhi EQU 4026 ; ring high tone
1045 3D09 ringon EQU 15625 ; ring ton = 2 s
1046 7A12 ringoff EQU 31250 ; ring toff = 4 s
1047 0032 busycount EQU 50 ; max # busy cycles
1048 0FBA busylow EQU 4026 ; busy low tone
1049 1451 busyhi EQU 5201 ; busy high tone
1050 0F42 busyon EQU 3906 ; busy ton = 0.5 s
1051 0F42 busyoff EQU 3906 ; busy toff = 0.5 s
1052 ;
1053 ;
1054
1055 0823 doapp
1056
1057 ; The following demonstration code sends the test_str
1058 ; string as DTMF signals. Tone on/off times are
1059 ; 40ms/40ms. Any SCI character received aborts
1060
1061 0823 TESTDTMF
1062 0823 CC0000 LDD #0
1063 0826 7C0806 STD ACFX ; clear phase accumulator
1064 0829 7C0808 STD ACFY ; clear phase accumulator
1065 082C 7C0804 STD tontimer ; clear tone timer
1066 082F 7C0800 STD DX ; init tone 1 (off)
1067 0832 7C0802 STD DY ; init tone 2 (off)
1068
1069 ; send a dial tone
1070
1071 0835 8644 LDAA #'D'
1072 0837 1608E9 JSR CPsub
1073
1074 ; send some DTMFs
1075
1076 083A CE085C LDX #test_str ; get test string
1077 083D 072B BSR DTMFstr ; send it
1078
1079 ; send ring back
1080
1081 083F 8652 LDAA #'R'
1082 0841 1608E9 JSR CPsub
1083

```

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```

1084                                     ; send busy
1085
1086    0844    8642    LDAA    #'B'
1087    0846    1608E9 JSR     CPsub
1088
1089    0849    CC0000 LDD     #0
1090    084C    7C0800 STD     DX
1091    084F    7C0802 STD     DY
1092    0852    86C0    LDAA    #\$C0
1093    0854    7A0806 STAA    ACFX
1094    0857    7A0808 STAA    ACFY
1095    085A    20FE L1BRA    L1                                     ; stop execution
1096
1097
1098    085C    392C35353537test_str FCB    "9,5557579,,,,",EOL
1099
1100                                     ; DTMFstr sends the string pointed at (X) as
1101                                     ; DTMF digits until EOL is detected.
1102                                     ; USES: A,B,X,Y
1103
1104    086A    A600 DTMFstr LDAA    0,X                                     ; get string character
1105    086C    08      INX
1106    086D    810D    CMPA    #EOL                                     ; end of string?
1107    086F    2704    BEQ     L2                                     ; yes,
1108    0871    0703    BSR     ASCdtmf                               ; send the tone
1109    0873    24F5    BCC     DTMFstr                               ; no interrupt,
1110    0875    3D L2 RTS
1111                                     ;
1112                                     ;
1113                                     ; ASCdtmf converts the ASCII in (A) to DTMF frequencies in DX
1114                                     ; & DY and times t-on. NON-DTMF characters result in a 0.5
1115                                     ; sec pause. DTMF characters are: {0-9}, {A-D}, {*}, and {#}
1116                                     ; USES: A,B,Y
1117
1118    0876    C7 ASCdtmf CLRB
1119    0877    CD08C9 LDY     #ASC_T                                     ; init table index
1120    087A    A140 L3CMPA    0,Y                                     ; in table?
1121    087C    270B    BEQ     gotASC                                  ; yes,
1122    087E    02      INY
1123    087F    52      INCB
1124    0880    C10F    CMPB    #maxDTMF                               ; end of table?
1125    0882    23F6    BLS     L3                                     ; no,
1126    0884    CC0F42 LDD     #halfsec                               ; delay 1/2 sec
1127    0887    2034    BRA     waitone
1128
1129
1130    0889    37 gotASC PSHB                                         ; save for later
1131    088A    C403    ANDB    #\$03                                   ; mask hi tone
1132    088C    58      LSLB                                         ; construct index (*2)
1133    088D    CD08E1 LDY     #DTMFhi
1134    0890    19ED    ABY
1135    0892    ED40    LDY     0,Y                                     ; get hi tone

```

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Application Note

```

1135 0894 7D0800 STY DX
1136 0897 33 PULB
1137 0898 C40C ANDB #\$0C ; mask low tone
1138 089A 54 LSRB ; = hinyb * 2
1139 089B CD08D9 LDY #DTMFlo
1140 089E 19ED ABY
1141 08A0 ED40 LDY 0,Y ; get low tone
1142 08A2 7D0802 STY DY
1143 08A5 CC04B0 LDD #toneon ; set on time
1144 08A8 7C0804 STD tontimer
1145 08AB 3E L4 WAI
1146 08AC FC0804 LDD tontimer
1147 08AF 26FA BNE L4 ; not done yet,
1148 08B1 CC0000 LDD #0 ; tones off
1149 08B4 7C0800 STD DX
1150 08B7 7C0802 STD DY
1151 08BA CC0258 LDD #toneoff ; set off time
1152 08BD 7C0804 waitone STD tontimer
1153 08C0 3E L5 WAI
1154 08C1 FC0804 LDD tontimer
1155 08C4 26FA BNE L5 ; not done yet,
1156 08C6 10FE CLC
1157 08C8 3D RTS
1158
1159 ; Table of ASCII DTMF digits
1160
1161 08C9 313233413435 ASC_T FCB "123A456B789C*0#D"
1162 000F maxDTMF EQU 15
1163
1164 ; table of high tones for each DTMF character.
1165 ; Tone values calculated from:
1166 ; D = (Fgen * 65536) / Fsamp = Fgen * 8.3886
1167
1168 08D9 16D5 DTMFlo FDB 5845 ; 697 Hz
1169 08DB 193B FDB 6459 ; 770 Hz
1170 08DD 1BEB FDB 7147 ; 852 Hz
1171 08DF 1ED6 FDB 7894 ; 941 Hz
1172
1173 08E1 279E DTMFhi FDB 10142 ; 1209 Hz
1174 08E3 2BC7 FDB 11207 ; 1336 Hz
1175 08E5 3066 FDB 12390 ; 1477 Hz
1176 08E7 3583 FDB 13699 ; 1633 Hz
1177 ;
1179 ;
1180 ;
1181 ; Cpsub uses (A) to select one of the following call
1182 ; progress tone pairs:
1183 ; (A) Signal state
1184 ; "D" dial tone (8 sec max)
1185 ; "R" ring back tone (100 rings)
1186 ; "B" Busy tone (50 burst cycles)

```

```

1187          ; USES: A,B,Y
1188
1189 08E9 D6C4 CPsub LDAB SC0SR1      ; preclear sci
1190 08EB D6C7      LDAB SC0DRL
1191 08ED 8144      CMPA #'D'        ; dial tone?
1192 08EF 262E      BNE nodial       ; no,
1193 08F1 CC0B78    LDD #dialow     ; set tones
1194 08F4 7C0800    STD DX
1195 08F7 CC0E6B    LDD #dialhi
1196 08FA 7C0802    STD DY
1197 08FD CCFFFF    LDD #$FFFF     ; set maximum duration
1198 0900 7C0804    STD tontimer
1199 0903 3E waitall WAI
1200 0904 96C4      LDAA SC0SR1
1201 0906 8520      BITA #RDRF
1202 0908 1401      SEC              ; preset SCI detect flag
1203 090A 2607      BNE killall     ; got an SCI chr,
1204 090C FC0804    LDD tontimer
1205 090F 26F2      BNE waitall    ; keep a' goin'...
1206 0911 10FE      CLC              ; clear SCI detect flag
1207 0913 96C7 killall LDAA SC0DRL
1208 0915 CC0000 LDD #0              ; turn off tones
1209 0918 7C0800 STD DX
1210 091B 7C0802 STD DY
1211 091E 3D RTS
1212
1213 091F 8152 nodial CMPA #'R'      ; ring-back tone?
1214 0921 262D BNE noring           ; no,
1215 0923 8632 LDAA #ringcount     ; set ring counter
1216 0925 7A080B STAA count
1217 0928 CC0E6B ringlp LDD #ringlow ; set tones
1218 092B 7C0800 STD DX
1219 092E CC0FBA LDD #ringhi
1220 0931 7C0802 STD DY
1221 0934 CC3D09 LDD #ringon       ; set ring on time
1222 0937 7C0804 STD tontimer
1223 093A 07C7 BSR waitall         ; wait...
1224 093C 2511 BCS CPexit         ; got an SCI, quit
1225 093E CC7A12 LDD #ringoff     ; set ring off time
1226 0941 7C0804 STD tontimer
1227 0944 07BD BSR waitall         ; wait again...
1228 0946 2507 BCS CPexit         ; got an SCI, quit
1229 0948 73080B DEC count        ; done 'em all yet?
1230 094B 26DB BNE ringlp         ; no,
1231 094D 10FE CLC                 ; no SCI detected
1232 094F 3D CPexit RTS
1233
1234 0950 10FE noring CLC           ; preclear SCI detect
1235 0952 8142 CMPA #'B'         ; busy tone?
1236 0954 26F9 BNE CPexit         ; no,
1237 0956 8632 LDAA #busycount    ; set ring counter

```

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Application Note

```

1238    0958    7A080B STAA    count
1239    095B    CC0FBA busylp LDD    #busylow           ; set tones
1240    095E    7C0800 STD     DX
1241    0961    CC1451 LDD     #busyhi
1242    0964    7C0802 STD     DY
1243    0967    CC0F42 LDD     #busyon           ; set ring on time
1244    096A    7C0804 STD     tontimer
1245    096D    0794    BSR     waitall           ; wait...
1246    096F    25DE    BCS     CPexit           ; got an SCI, quit
1247    0971    CC0F42 LDD     #busyoff          ; set ring off time
1248    0974    7C0804 STD     tontimer
1249    0977    078A    BSR     waitall           ; wait again...
1250    0979    25D4    BCS     CPexit           ; got an SCI, quit
1251    097B    73080B DEC     count           ; done 'em all yet?
1252    097E    26DB    BNE     busylp           ; no,
1253    0980    10FE    CLC           ; no SCI detected
1254    0982    3D     RTS

```

Sine Table Generator C Program

```

#include <stdio.h>
#include <math.h>

// This program constructs a sine table as specified by the user.
// min, max, and size are provided at run time with the output
// going to the display and a file named "SINE.ASM."
//
// Table entries are defined by the following:
// sin,x = int(MIDP + (swing * SIN (360 * x / 256)))
//
// where x = table offset

FILE *fi;
float max = 255;
float min = 1;
float size = 256;
const float pie = 3.141592654;
float x, y, MIDP, SWING, t;

void main(void)

{

```

```

printf("Sine table compiler, v1.00\n");
printf("Sending output to \"SINE.ASM\"...\n");
if ( (fi = fopen("SINE.ASM", "w")) != NULL)
    {
        // get table parameters

        printf("Enter table size (256 max): ");
        scanf("%f", &size);
        printf("Enter table min value (0-255): ");
        scanf("%f", &min);
        printf("Enter table max value (0-255): ");
        scanf("%f", &max);
        SWING = (max - min) / 2;
        MIDP = min + SWING;


        // put descriptor header in .asm file

        printf("; sine lookup table\n");
        fprintf(fi, "; sine lookup table\n");
        printf("; size = %5.0f, min = %5.0f, max = %5.0f \n", size, min, max);
        fprintf(fi, "; size = %5.0f, min = %5.0f, max = %5.0f \n", size, min, max);
        printf("; MID = %f    SWING = %f\n", MIDP, SWING);
        fprintf(fi, "; MID = %f    SWING = %f\n", MIDP, SWING);
        fprintf("SIN_TAB\n");// place table lable

        // put table data as assembly source.

        x = 0;
        while (x <= size)
            {
                y = MIDP + (SWING * (sin (2 * pie * x / size)));
                printf("\tFCB\t");// display source
                printf("%5.0f", y);
                printf("\n");
                fprintf(fi, "\tFCB\t");// write source file
                fprintf(fi, "%5.0f", y);// for casm0x use "%5.0ft"
                fprintf(fi, "\n");
                x++;
            }
        fclose(fi);
        printf("Done.\n");
    }
else
    {
        printf("File error.\n");
    }
}

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